



A NOVEL STABILITY CONDITION AND ITS APPLICATION TO GA-BASED FUZZY CONTROL FOR NONLINEAR SYSTEMS WITH UNCERTAINTY

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A NOVEL STABILITY CONDITION AND ITS APPLICATION TO GA-BASED FUZZY CONTROL FOR NONLINEAR SYSTEMS WITH UNCERTAINTY

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Key words: modified adaptive fuzzy sliding mode control, Lyapunov direct method, genetic algorithm.

ABSTRACT

In this study, we strive to combine the advantages of fuzzy logic control (FLC), genetic algorithms (GA), H_∞ tracking control schemes, smooth control and adaptive laws to design an adaptive fuzzy sliding model controller for the rapid and efficient stabilization of complex and nonlinear systems. First, we utilize a reference model and a fuzzy model (both involving FLC rules) to describe and well-approximate an uncertain, nonlinear plant. The FLC rules and the consequent parameter are decided on via GA. A boundary-layer function is introduced into these updated laws to cover modeling errors and to guarantee that the state errors converge into a specified error bound. After this, a H_∞ tracking problem is characterized. We solve an eigenvalue problem (EVP), and derive a modified adaptive neural network controller (MANN) to simultaneously stabilize and control the system and achieve H_∞ control performance. Furthermore, a stability criterion is derived utilizing Lyapunov's direct method to ensure the stability of the nonlinear system. Finally, the control methodology is demonstrated via a numerical simulation.

I. INTRODUCTION

Over the past few years, there has been significant research efforts devoted to the analysis and control designs of fuzzy systems (see [2], [32], [34] and the references therein). The main motivation for this development has been applications to practical nonlinear systems and engineering problems (see [4, 10, 13, 15, 17, 24, 25, 27, 29, 30, 31, 37] and the references

therein). Undoubtedly, the Lyapunov theory is one of the most common approaches for dealing with the stability analysis of systems. However to overcome the conservatism that arises from the use of Lyapunov methods it has been necessary to develop a number of more effective methods, for example, fuzzy Lyapunov functions [8], [35]. There are also many important issues that have required studied for T-S fuzzy control systems, such as time delays [4, 7, 9, 26, 42], H_∞ performance [11, 20], robustness [23, 41], neural networks (NN) and genetic algorithms (GA) [5, 14, 18, 28]. It should be noted that most of the aforementioned research efforts have been focused on PDC laws. Until now, how to integrate control theory and non-PDCs law into practical engineering computations has been an open question.

As has been explored in previous research, an adaptive algorithm can be adopted to find the best high-performance parameters for the fuzzy sliding mode controller (FSMC) [39], [40] for nonlinear control problems [19], [39]. Adaptive laws are devised afterwards to adjust the parameters of the fuzzy models, including the design of the adaptive fuzzy sliding mode controller (AFSMC) [43]. This is a powerful and robust control strategy for dealing with uncertainties and external disturbances.

Aside from the above, it is also very important to decide on the fuzzy rules and the initial values of the parameter vector values for the AFSMC. A GA [16], [22] is usually used as an optimization technique in the self-learning or training strategy for deciding on the fuzzy control rules and the initial values of the parameter vector. Using this GA-based AFSMC improves the immediate response, stability, and robustness of the control system. A new *Lyapunov* stability criterion needs to be developed for the H_∞ tracking performance throughout all the system states to be considered in the proposed control strategy [3]. Based on the *Lyapunov* theory [33], it can be shown that the proposed controller guarantees good H_∞ tracking performance throughout the entire system states.

Another common problem encountered when switching the control input of the sliding model system is the so-called "chattering" phenomenon [38]. The smoothing of control discontinuity inside a thin boundary layer essentially acts as a low-pass filter structure for the local dynamics. This eliminates chattering, to guarantee that the state errors converge within a specified error bound.

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This study focuses on designing a robust tracking control for a class of nonlinear system involving plant uncertainties and external disturbances. To achieve this task, H_∞ tracking control is incorporated into the AFSMC, to produce the proposed H_∞ AFSMC design. It is shown that the proposed controller can guarantee H_∞ tracking performance throughout the entire system states, based on the *Lyapunov* theory [33]. The *Lyapunov* stability condition is transformed into the form of a certain linear matrix inequality (LMI) problem [1, 21, 36] which allows one to efficiently obtain the parameters of the controller by using the convex optimization techniques to solve either the EVP or the LMI problem.

II. REFERENCE MODELING FOR NONLINEAR DYNAMIC SYSTEMS

The plant is a single-input/single-out n th-order system with $n \geq 1$.

$$y^{(n)} = f(x) + g(x) \cdot u + d(t) \tag{1}$$

The system is said to have a relative degree n , if $g(x)$ is bounded away from zero.

Assumption 1: $g(x)$ is bounded away from zero over a compact set $\zeta \subset R^n$, $|g(x)| \geq b > 0, \forall x \in \zeta$.

$$r = y_r + \alpha_{n-1} y_r^{(n-1)} + \alpha_{n-2} y_r^{(n-2)} + \dots + \alpha_1 \dot{y}_r + \alpha_0 y_r \tag{2}$$

where $\alpha_{n-1}, \dots, \alpha_1, \alpha_0$ are chosen such that the polynomial $\ell^n + \alpha_{n-1} \ell^{n-1} + \dots + \alpha_1 \ell + \alpha_0$ is Hurwitz; and ℓ here denotes the *Laplace* variable. If $f(x), g(x)$ are known, and **Assumption 1** is satisfied, the control law can be defined by

$$u = \frac{-f(x) - d(x) - \left(\alpha_{n-1} y^{(n-1)} + \dots + \alpha_1 \dot{y} + \alpha_0 y \right) + r}{g(x)}, \tag{3}$$

$\forall x \in S$

Substituting (3) into (1), the linearized system becomes

$$(y_r - y)^{(n)} + \alpha_{n-1} (y_r - y)^{(n-1)} + \dots + \alpha_1 (\dot{y}_r - \dot{y}) + \alpha_0 (y_r - y) = 0 \tag{4}$$

If we define $e = y_r - y$ as the tracking error, then the reference control input (2) results in the following error equation:

$$e^{(n)} + \alpha_{n-1} e^{(n-1)} + \dots + \alpha_1 \dot{e} + \alpha_0 e = 0 \tag{5}$$

III. GA-BASED H_∞ MAFSMC FOR NONLINEAR SYSTEMS

The control objective can be achieved by the control law

$$u = u_{eq} + u_d \tag{6}$$

where u_{eq} is equivalent control. Now let

$$u_d = -g(x)^{-1} \frac{1}{\rho} |S| \cdot \text{sat}(S/\Phi) \tag{7}$$

The thin boundary layer function $\text{sat}(S/\Phi)$ is defined as

$$\text{sat}(S/\Phi) = \begin{cases} 1, & \text{if } (S/\Phi) > 1 \\ (S/\Phi), & \text{if } -1 \leq (S/\Phi) \leq 1 \\ -1, & \text{if } (S/\Phi) < -1 \end{cases}$$

We can utilize the certainty equivalent control approach [40] to design an FLC (8) to approximate u_{eq}

$$\bar{u}_{eq}(\bar{\theta}) = \sum_{k=1}^m R_k \left(-\left(\frac{\|S - C_k\|}{\beta} \right)^2 \right) \cdot \bar{\theta}_k \tag{8}$$

where m is the sum of the fuzzy rules; $\bar{\theta}_k, i.e., |\bar{\theta}_k| \leq \theta_{\max}$ are adjustable consequent parameters of FLC; and $R(S) = [R_1(S), R_2(S), \dots, R_m(S)]^T$ is the vector of the fuzzy basis function [31] defined as

$$R_k = \frac{\mu_k(S - C_k)}{\sum_{k=1}^m \mu_k(S - C_k)}, \tag{9}$$

$$\mu_k(\|S - C_k\|) = \exp \left(-\left(\frac{\|S - C_k\|}{\beta} \right)^2 \right)$$

Assumption 2:

For $x \in \zeta \subset R^n$, there exists an adjustable parameter vector $\bar{\theta} = [\bar{\theta}_1, \bar{\theta}_2, \dots, \bar{\theta}_n]^T$ such that the fuzzy system $\bar{u}(S, \bar{\theta}) = \bar{\theta}^T R(S)$ can approximate the continuous function u with accuracy ϵ_{\max} over the set ζ , that is, $\exists \bar{\theta}$ such that

$$\sup \left| \bar{u}_{eq}(S, \bar{\theta}) - u_{eq}(S) \right| \leq \epsilon_{\max}, \forall S \in \zeta \tag{10}$$

Let $\hat{\theta}$ denote the estimative of $\bar{\theta}$ at time t . Then, define the estimative control output $\hat{u}_{eq}(S, \hat{\theta})$ as

$$\hat{u}_{eq}(S, \hat{\theta}) = \sum_{k=1}^m \hat{\theta}_k \cdot R_k(S) = \hat{\theta}^T R(S) \quad (11)$$

If the parameter error vector at time t is $\tilde{\theta} = \bar{\theta} - \hat{\theta}$, then,

$$\tilde{\theta}^T R(S) = \bar{u}_{eq}(S, \bar{\theta}) - \hat{u}_{eq}(S, \hat{\theta}) \quad (12)$$

From **Assumption 2**, define the modeling error as follows:

$$\varepsilon = u_{eq} - \bar{u}_{eq}(S, \bar{\theta}), \text{ where } |\varepsilon| \leq \varepsilon_{\max} \quad (13)$$

We can now say

$$u_{eq} = \hat{u}_{eq}(S, \hat{\theta}) + \tilde{\theta}^T R(S) + \varepsilon \quad (14)$$

Then, substituting (7) and (14) into (3), we can obtain the error dynamic equation from

$$\begin{aligned} & e + \alpha_{n-1} e^{(n-1)} + \dots + \alpha_1 \dot{e} + \alpha_0 e \\ &= g(x) \cdot (\tilde{\theta}^T R(S) + \varepsilon) - \frac{1}{\rho} |S| \cdot \text{sat}(S/\Phi) \end{aligned} \quad (15)$$

Define the augmented error as

$$S = \beta_{n-1} e^{(n-1)} + \dots + \beta_1 \dot{e} + \beta_0 e \quad (16)$$

where $\beta_{n-1}, \dots, \beta_1, \beta_0$ in (15); and $\alpha_{n-1}, \dots, \alpha_1, \alpha_0$ in (14) are chosen such that

$$\hat{M}(\ell) = \frac{\beta_{n-1} \ell^{n-1} + \dots + \beta_1 \ell + \beta_0}{\ell^n + \alpha_{n-1} \ell^{n-1} + \dots + \alpha_1 \ell + \alpha_0} = \frac{N(\ell)}{D(\ell)} \quad (17)$$

is SPR (strictly positive real) transfer function, and $N(\ell)$ and $D(\ell)$ are coprime.

Define $e_m = \begin{bmatrix} e, \dot{e}, \dots, e^{(n-1)} \end{bmatrix}^T$ as the states for (16) which can be realized as

$$\dot{e}_m(t) = \Lambda \cdot e_m(t) + b \cdot \left[g(x) \cdot (\tilde{\theta}^T R(S) + \varepsilon) - \frac{1}{\rho} |S| \cdot \text{sat}(S/\Phi) \right] \quad (18)$$

$$S(t) = c^T e_m(t) \quad (19)$$

Where

$$\Lambda = \begin{bmatrix} 0 & 1 & 0 & \dots & 0 & 0 \\ 0 & 0 & 1 & \dots & 0 & 0 \\ \vdots & \vdots & \vdots & \ddots & \vdots & \vdots \\ 0 & 0 & 0 & \dots & 1 & 0 \\ 0 & 0 & 0 & \dots & 0 & 1 \\ -\alpha_0 & -\alpha_1 & -\alpha_2 & \dots & -\alpha_{n-2} & -\alpha_{n-1} \end{bmatrix}_{n \times n}, b = \begin{bmatrix} 0 \\ 0 \\ \vdots \\ 0 \\ 0 \\ 1 \end{bmatrix}_{n \times 1}$$

$$c = [\beta_0 \ \beta_1 \ \dots \ \beta_{n-1}]^T, \text{ let } \beta_{n-1} = 1.$$

Observing (19), it is clear that the lumped uncertainty $\omega = g(x) \cdot \varepsilon$ directly affects the tracking error. To achieve the control objective, the following H_∞ tracking performance related to the tracking error vector e_m is requested [36]:

$$\int_0^T e_m^T Q e_m dt \leq e_m^T(0) P e_m(0) + \frac{1}{\gamma} \tilde{\theta}^T(0) H_{11} \tilde{\theta}(0) + \rho^2 \int_0^T \omega^2 dt \quad (20)$$

for all $\omega \in L_2[0, T], \forall T \in [0, \infty)$, where Q and P are symmetric positive definite weighting matrices; and $0 < \rho < 1$ is a prescribed attenuation level.

It is seen that if the system starts with the initial conditions $e_m(0) = 0, \tilde{\theta}(0) = 0$, then the H_∞ tracking performance of (21) becomes

$$\int_0^T e_m^T Q e_m dt \leq \rho^2 \int_0^T \omega^2 dt \quad (21)$$

That is, the L_2 -gain from ω to e_m must be equal to or less than a prescribed value ρ [36]. The following results can be obtained:

Theorem 1: Consider the nonlinear uncertain system $y^{(n)} = f(x) + g(x) \cdot u + d$ that satisfies Assumptions $(\bar{\theta}, \hat{\theta})$. Suppose that the unknown control input u which is approximated by $\hat{u}_{eq}(S, \hat{\theta})$ by (11), S is given by (17), Q is a symmetric positive definite weighting matrix, and $0 < \rho < 1$ is the design constant serving as an attenuation level.

Let $K = K^T > 0$ be the solution of the following LMI:

$$\Lambda^T K + K \Lambda + \frac{1}{\rho} K b b^T K - \frac{1}{\rho} c c^T + \frac{1}{\rho} Q \leq 0 \quad (22)$$

and define $P = c c^T + K$. The control law chosen is $u_{eq}(S, \hat{\theta})$

and the modified adaptive laws are given by

$$\dot{\hat{\theta}} = \gamma \cdot |S| \cdot \text{sat}(S/\Phi) R + \gamma \cdot b^T K e_m R \quad (23)$$

in which $\gamma > 0$ is the adaptive gain. The H_∞ tracking performance of (21) for the overall system can be guaranteed.

Proof:

The time derivative of S can be obtained by

$$\dot{S} = c^T \dot{e}_m(t) = c^T \{ \Lambda \cdot e_m(t) + b \cdot [g(x) \cdot (\tilde{\theta}^T R(S) + \varepsilon) - \frac{1}{\rho} |S| \cdot \text{sat}(S/\Phi)] \} \quad (24)$$

Now, we shall investigate the stability of the origin using *Lyapunov* function candidates. The *Lyapunov* function candidate of the state is defined as follows:

$$V = \frac{1}{2} e_m^T P e_m + \frac{1}{2\gamma} \tilde{\theta}^T H \tilde{\theta} \quad (25)$$

where γ is a positive constant representing the learning rate,

$$\tilde{\theta} = [\tilde{\theta}_1 \ \tilde{\theta}_2 \ \dots \ \tilde{\theta}_m]^T, \quad H = g(x) \cdot I_{m \times m},$$

because $P = cc^T + K$, (26) can be expressed as

$$\begin{aligned} V &= \frac{1}{2} e_m^T (cc^T + K) e_m + \frac{1}{2\gamma} \tilde{\theta}^T H \tilde{\theta} \\ &= \frac{1}{2} (S^2 + e_m^T K e_m) + \frac{1}{2\gamma} \tilde{\theta}^T H \tilde{\theta} \end{aligned}$$

The time derivative of V can be described as

$$\begin{aligned} \dot{V} &= S\dot{S} + \frac{1}{2} \dot{e}_m^T K e_m + \frac{1}{2} e_m^T K \dot{e}_m + \frac{1}{\gamma} \tilde{\theta}^T H \dot{\tilde{\theta}} \\ &= S \cdot [g(x) \cdot \tilde{\theta}^T R(S)] + S \cdot [g(x) \cdot \varepsilon] - \frac{1}{\rho} S^2 \\ &\quad + \frac{1}{2} e_m^T (\Lambda^T K + K \Lambda) e_m + [g(x) \cdot (\tilde{\theta}^T R(S) + \varepsilon) \\ &\quad - \frac{1}{\rho} |S| \cdot \text{sat}(S/\Phi)] \cdot b^T K e_m + \frac{1}{\gamma} \tilde{\theta}^T H (-\dot{\tilde{\theta}}) \end{aligned} \quad (26)$$

Substituting the adaptive laws (24) into (27), and when $|S| > \Phi$, we derive

$$\begin{aligned} \dot{V} &= S \cdot \omega - \frac{1}{\rho} S^2 + \frac{1}{2} e_m^T (\Lambda^T K + K \Lambda) e_m + \omega \cdot b^T K e_m \\ &\quad - \frac{1}{\rho} S \cdot b^T K e_m \end{aligned} \quad (27)$$

(27) can now be rewritten as

$$\begin{aligned} \dot{V} &= \omega \cdot (S + b^T K e_m) - \frac{1}{\rho} S^2 + \frac{1}{2} e_m^T (\Lambda^T K + K \Lambda) e_m - \frac{1}{\rho} S \cdot b^T K e_m \\ &= -[\frac{1}{\sqrt{2}} \sqrt{\rho} \cdot \omega - \frac{1}{\sqrt{2\rho}} (S + b^T K e_m)]^2 + \frac{1}{2} \rho \omega^2 \\ &\quad + \frac{1}{2\rho} (S + b^T K e_m)^2 - \frac{1}{\rho} S^2 + \frac{1}{2} e_m^T (\Lambda^T K + K \Lambda) e_m \\ &\quad - \frac{1}{\rho} S \cdot b^T K e_m \\ &= -[\frac{1}{\sqrt{2}} \sqrt{\rho} \cdot \omega - \frac{1}{\sqrt{2\rho}} (S + b^T K e_m)]^2 + \frac{1}{2} \rho \omega^2 \\ &\quad + \frac{1}{2\rho} (S^2 + 2Sb^T K e_m + e_m^T K b b^T K e_m) \\ &\quad - \frac{1}{\rho} S^2 + \frac{1}{2} e_m^T (\Lambda^T K + K \Lambda) e_m - \frac{1}{\rho} S \cdot b^T K e_m \\ &\leq \frac{1}{2} e_m^T (\Lambda^T K + K \Lambda + \frac{1}{\rho} K b b^T K) e_m - \frac{1}{2\rho} S^2 + \frac{1}{2} \rho \omega^2 \\ &= \frac{1}{2} e_m^T (\Lambda^T K + K \Lambda + \frac{1}{\rho} K b b^T K - \frac{1}{\rho} c c^T) e_m + \frac{1}{2} \rho \omega^2 \end{aligned} \quad (28)$$

From (22),

$$\dot{V} \leq -\frac{1}{2\rho} e_m^T Q e_m + \frac{1}{2} \rho \omega^2 \quad (29)$$

Integrating both sides of (28) yields

$$V(t_f) - V(0) \leq -\frac{1}{2\rho} \int_0^{t_f} e_m^T Q e_m dt + \frac{\rho}{2} \int_0^{t_f} \omega^2 dt \quad (30)$$

Thus,

$$\int_0^{t_f} e_m^T Q e_m dt \leq 2\rho V(0) - 2\rho V(t_f) + \rho^2 \int_0^{t_f} \omega^2 dt$$

Since $0 < \rho < 1$ and $V \geq 0$, (31) can be rewritten as

$$\int_0^{t_f} e_m^T Q e_m dt \leq 2V(0) + \rho^2 \int_0^{t_f} \omega^2 dt$$

With (25), the following result can be obtained:

$$\int_0^{t_f} e_m^T Q e_m dt \leq e_m^T(0) P e_m(0) + \frac{1}{\gamma} \tilde{\theta}^T(0) H_{11} \tilde{\theta}(0) + \rho^2 \int_0^{t_f} \omega^2 dt \quad (31)$$

So, the H_∞ tracking performance in (18) is achieved. This completes the proof.

Note that the matrix inequalities in (22) can be transformed into a certain form of LMI. That is, by the Schur complements [1], (22) is equivalent to

$$\begin{bmatrix} \Lambda^T K + K \Lambda - \frac{1}{\rho} c c^T & K b & Q^{1/2} \\ b^T K & -\rho & 0_{1 \times n} \\ (Q^{1/2})^T & 0_{n \times 1} & -\rho \cdot I_{n \times n} \end{bmatrix} \leq 0 \quad (32)$$

where $(Q^{1/2})^T Q^{1/2} = Q$. Therefore, the minimization problem can be formulated as the following eigenvalue problem (EVP): subject to $K_i = K_i^T > 0$ and (32).

IV. NUMERICAL SIMULATION

The active TMD mounted on a shear structure is modeled as a Four-degree-of freedom structure-ATMD system, as shown in Fig. 1 ATMD System. The parameters with ATMD: $m_d = 50$ (kg), $c_d = 14.05$ (N-s/m), and $k_d = 9875.18$ (N/m) represent mass, damping, and stiffness, and the parameter vectors: M_{ST} (kg), $C_{ST}(t)$ (N-s/m), and $K_{ST}(t)$ (N/m) represent the mass, uncertain damping, and uncertain stiffness vectors, respectively, ($t = t + \Delta t$, $\Delta t = 0.02$ sec) of this dilapidated-simulation structure with ATMD shown below. F and u represent the external force and control input. The dynamic equations of motion of the pendulum are given below.

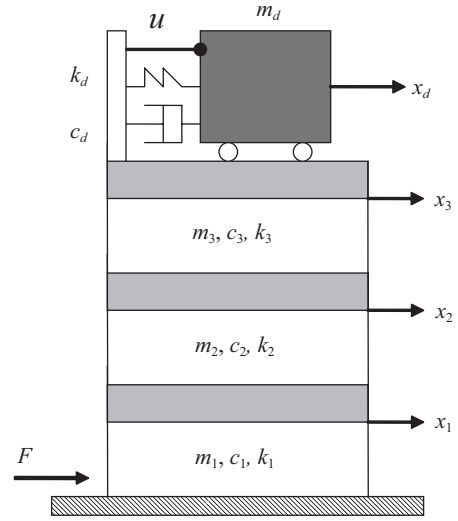


Fig. 1. Four-DOF structure-ATMD system.

$$K_{ST}(t) = \begin{bmatrix} 2740599(1-0.3t) & -1640938(1-0.3t) & 368992(1-0.3t) & 0 \\ -1640938(1-0.3t) & 3020937(1-0.3t) & -1624126(1-0.3t) & 0 \\ 368992(1-0.3t) & -1624126(1-0.3t) & 1333065(1-0.3t) + 9875.2 & -9875.2 \\ 0 & 0 & -9875.2 & 9875.2 \end{bmatrix}$$

$$C_{ST}(t) = \begin{bmatrix} 382.65(1+0.1t) & -57.27(1+0.1t) & 61.64(1+0.1t) & 0 \\ -57.27(1+0.1t) & 456.73(1+0.1t) & -2.63(1+0.1t) & 0 \\ 61.64(1+0.1t) & -2.63(1+0.1t) & 437.29(1+0.1t) + 14.05 & -14.05 \\ 0 & 0 & -14.05 & 14.05 \end{bmatrix}$$

$$\begin{bmatrix} \ddot{x}_1 \\ \ddot{x}_2 \\ \ddot{x}_3 \\ \ddot{x}_d \end{bmatrix} = \begin{bmatrix} (-M^{-1}K_{ST})_{4 \times 4} & (-M^{-1}C_{ST})_{4 \times 4} \end{bmatrix} \begin{bmatrix} x_1 \\ x_2 \\ x_3 \\ x_d \\ \dot{x}_1 \\ \dot{x}_2 \\ \dot{x}_3 \\ \dot{x}_d \end{bmatrix} + \begin{bmatrix} 0 \\ 0 \\ -1/m_3 \\ -1/m_d \end{bmatrix} \cdot u + \begin{bmatrix} -1/m_1 \\ -1/m_2 \\ -1/m_3 \\ -1/m_d \end{bmatrix} \cdot F \quad (33)$$

where $M_{ST} = \begin{bmatrix} 980.71 & 0 & 0 & 0 \\ 0 & 980.71 & 0 & 0 \\ 0 & 0 & 980.71 & 0 \\ 0 & 0 & 0 & 50 \end{bmatrix}$,

The design procedure for the GA-based H_∞ -MAFSMC analyzed above can be summarized as follows:

[Step 1] In the simulation we set the sensor on the top floor of a dilapidated structure. Using the procedure discussed above, we specify the response of the control system by defining suitable sliding surface $S = c^T e_m = 30e_3 + \dot{e}_3$, then, construct the structure of the MAFSMC based on GA and the initial values of the consequent parameter vector $\hat{\theta}$ chosen as follows: [1 0.9 0.65 0.30 0.05 0 -0.06 -0.25 -0.33 -0.7 -0.95]’.

[Step 2] Let $Q = I_{2 \times 2}$, with the specified attenuation level $\rho = 0.5$. Now we use the LMI optimization toolbox in Matlab [21] to solve the EVP in (32), to obtain $K = \begin{bmatrix} 232.4346 & -13.2239 \\ -13.2239 & 2.7998 \end{bmatrix}$

and $P = c c^T + K = \begin{bmatrix} 1132.4346 & 16.7761 \\ 16.7761 & 3.7998 \end{bmatrix}$.

[Step 3] Apply the controller, as given in (7) and (14), to control the nonlinear system (1). Next, we let $\gamma = 0.05$, $\Phi = 0.2$, and adjust $\hat{\theta}$ by the adaptive law, as given by (23).

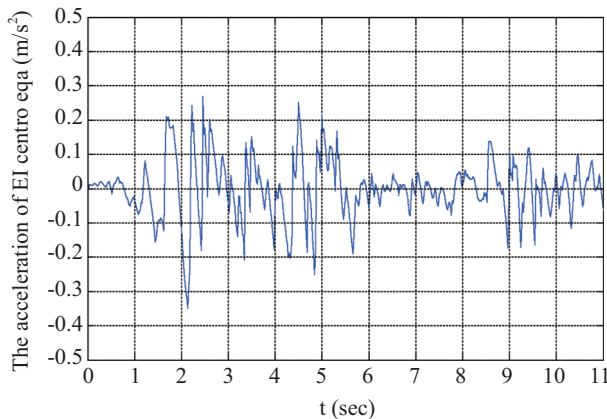


Fig. 2. Acceleration of the El Centro earthquake.

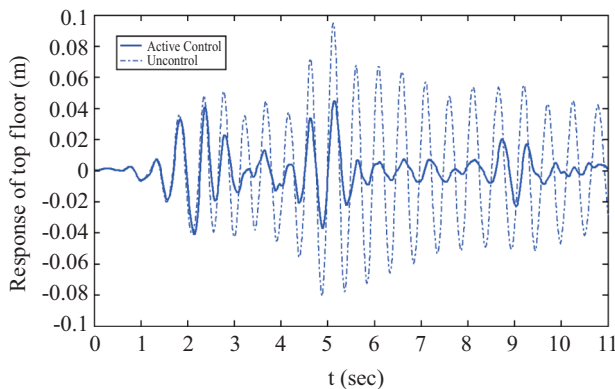


Fig. 3. Top floor response of the structure in the El Centro earthquake.

An examination of the simulation results for the El Centro earthquake disturbances, illustrated in Figs. 2-3, shows an improvement in the performance of the system in all respects while retaining the advantage of robustness in the presence of bounded disturbances.

Figures 2-3 show that the dilapidated structure simulation is rapidly stable and the GA-based H_∞ -MAFSMC can be derived to stabilize and control the system.

V. CONCLUSIONS

A GA-based H_∞ modified adaptive fuzzy sliding model controller for the handling the nonlinear systems is described in this paper. We first track the reference trajectory to approximate an uncertain and nonlinear plant via fuzzy model involving FLC rules. Then, we utilize a GA to decide on the initial values of the consequent parameter vector $\hat{\theta}$. The H_∞ tracking problem is characterized in terms of solving an eigenvalue problem. The smoothing of control discontinuities inside a thin boundary layer, essentially as a low-pass filter structure, is introduced into these updated laws for the elimination of chattering and to guarantee that the state errors

converge within a specified error bound. Next, an MAFSMC is proposed to stabilize the system, and achieve H_∞ control performance at the same time. A stability criterion is also derived from *Lyapunov's* direct method to ensure the stability of the nonlinear system. The stability analysis can thus be reduced into LMI problems. Finally, we discuss an example, a numerical simulation. We demonstrate that the control methodology can rapidly and efficiently control an uncertain and nonlinear system.

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